

Power-and Rate-Adaptation Improves the Effective Capacity of C-RAN for Nakagami- m Fading Channels

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Abstract—We propose a power-and rate-adaptation scheme for cloud radio access networks (C-RANs), where each radio remote head (RRH) is connected to the baseband unit (BBU) pool through optical links. The RRHs jointly support the users by efficiently exploiting the enhanced spatial degrees of freedom. Our proposed scheme aims for maximizing the effective capacity (EC) of the user subject to both per-RRH average-and peak-power constraints, where the EC is defined as the maximum arrival rate that can be supported by the C-RAN under the statistical delay requirement. We first transform the EC maximization problem into an equivalent convex optimization problem. By using the Lagrange dual decomposition method and solving the Karush-Kuhn-Tucker (KKT) equations, the optimal transmission power of each RRH can be obtained in closed-form. Furthermore, an online tracking method is provided for approximating the average power of each RRH. For the special case of two RRHs, the expression of the average power of each RRH can be calculated in explicit form. Hence, the Lagrange dual variables can be computed in advance in this special case. Furthermore, we derive the power allocation for two important extreme cases: 1) no delay constraint; 2) extremely stringent delay-requirements. Our simulation results show that the proposed scheme significantly outperforms the conventional algorithm without considering the delay requirements. Furthermore, when appropriately tuning the value of the delay exponent, our proposed algorithm is capable of guaranteeing a delay outage probability below 10^{-9} when the maximum tolerable delay is 1 ms. This is suitable for the future ultra-reliable low latency communications (URLLC).

Index Terms—URLLC, Effective capacity, Delay constraints, Cross-layer design, C-RAN.

I. INTRODUCTION

The fifth-generation (5G) wireless system to be deployed by 2020 is expected to offer a substantially increased capacity [1]. To achieve this ambitious goal, the C-RAN concept has been regarded as one of the most promising solutions. In particular, C-RAN is composed of three key components: 1) a pool of BBUs centrally located at a cloud data center; 2) low-cost, low-power distributed RRHs deployed in the network; 3) high-bandwidth low latency fronthaul links that connect the RRHs

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to the BBU pool. Under the C-RAN architecture, most of the baseband signal processing of conventional base stations has been shifted to the BBU pool and the RRHs are only responsible for simple transmission/reception functions, some of the hitherto centralized signal processing operations can be relegated to the BBU pool. Hence, the network capacity can be significantly improved.

Recently, the performance of C-RAN has been extensively studied [2]–[5], albeit these papers have been focused on the physical layer issues, which giving no cognizance to the delay of the upper layer’s. However, most of the multimedia services, such as video conferencing and mobile TV have stringent delay requirements. Due to the time-varying characteristics of fading channels, it is impossible to impose a deterministic delay-bound guarantee for wireless communications. For the sake of analyzing the statistical QoS performance, Wu *et al.* [6] introduced the notion of effective capacity (EC), which can be interpreted as the maximum constant packet arrival rate that can be supported by the system, whilst satisfying a maximum buffer-violation probability constraint.

Due to the complex expression of EC, most of the existing papers focus on the EC maximization problem for the simple scenario, where there is only a single transmitter [7]–[11]. Specifically, a QoS-driven power-and rate-adaptation scheme was proposed for single-input single-output (SISO) systems communicating over flat-fading channels in [7], with the objective of maximizing EC subject to both delay-QoS and average power constraints, which is characterized by the QoS exponent θ . A smaller θ corresponds to a looser QoS guarantee, while a higher value of θ represents a more stringent QoS requirement. The results of [7] showed that in the extreme case of $\theta \rightarrow 0$, the power allocation reduces to the conventional water-filling solution. By contrast, when $\theta \rightarrow \infty$, the optimal power allocation becomes the channel inversion scheme, where the system operates under a fixed transmission rate. The EC maximization problem was studied in [8] in the context of cognitive radio networks, where the power constraints of [7] were replaced by the maximum tolerable interference-power at the primary user. Closed-form expressions of both the power allocation and the EC were derived for the secondary user. The power minimization problem subject to EC constraints was considered in [9] for three different scenarios. Significant power savings can be achieved by using the power allocation scheme of [9]. To a further advance, both subcarrier and power allocation were investigated in [10] for a one-way relay

network wherein the optimal subcarrier and power allocation was derived by adopting the Lagrangian dual decomposition method. Most recently, Wenchi *et al.* [11] considered both the average-and peak-power constraints when maximizing the EC, and provided the specific conditions, when the peak power constraints can be removed. From the information-theoretical point of view, it is difficult to solve the ergodic capacity maximization problem subject to both the average-and peak-power constraints, even for the basic Gaussian white noise channel. In Shannon's landmark paper [12], only the asymptotically low and high SNR for the bandlimited continuous time Gaussian channel was studied. This problem was later studied by Smith [13] and showed that the capacity achieving distribution is discrete. In [14], the authors considered the more general case of the quadrature additive Gaussian channel and derived the lower and upper bounds of this channel's capacity. Khojastepour *et al.* [15] studied the capacity of the fading channel under both types of power constraints under the assumption of the perfect channel state information available at both the transmitter and receiver side. However, the above papers [12]–[14] neither consider the upper layer delay nor the multiple transmission points.

To avoid any traffic congestion and attain a good C-RAN performance, the adaptive power allocation scheme should take the diverse QoS requirements into account to guarantee the satisfaction of users. In this paper, we aim for jointly optimizing the power allocation of each RRH in order to maximize the EC of a user of the C-RAN, where both the average power and peak power constraints of each RRH are considered. This user is jointly served by all RRHs of the C-RAN due to the powerful computational capability of the BBU pool. Unfortunately, the power allocation schemes developed in the aforementioned papers for single-transmitter scenarios [7]–[11] cannot be directly applied to C-RAN's relying on multiple RRHs for serving the user and to simultaneously exploit the spatial degrees of freedom. The reason can be explained as follows. In these papers, there is only a single transmitter and only a sum-power constraint is imposed. The Lagrange method can be used to find the optimal power allocation, which is in the form of a water-filling-like solution in general. However, for the C-RAN, all RRHs have their individual power constraints and the power cannot be shared among the RRHs. Yu *et al.* [16] provided a detailed reason as to why the classic Lagrange method cannot be readily applied in C-RAN. Hence, new methods have to be developed. Specifically, the contributions of this paper can be summarized as follows:

1) In this paper, we derive the optimal power allocation for each RRH by resorting to the Lagrangian dual decomposition and the Karush-Kuhn-Tucker (KKT) conditions. The power allocation solutions depend both on the user's QoS requirements and on the joint channel conditions of the RRHs.

2) The Lagrangian dual decomposition requires us to calculate the subgradient, where the average power of each iteration should be obtained. However, it is numerically challenging to derive the expression of average power for each RRH. To tackle this issue, we provide an online training method for tracking the average power of each RRH. For the special case

TABLE I
THE LIST OF NOTATIONS

I	The number of RRHs
\mathcal{I}	The set of RRHs
T_f	The time frame length
m	Nakagami parameter
α_i	Channel-power-to-noise ratio (CPNR)
θ	QoS exponent
$EC(\theta)$	The effective capacity specified by θ
μ	Constant arrival data rate
D_{\max}	Maximum delay bound
B	System bandwidth
P_i^{avg}	Average power constraint of RRH i
P_i^{peak}	Peak power constraint of RRH i

of a single RRH, the closed-form expression of average power can be obtained. For the more complex case of two RRHs, we also provide the expression of the average power for each RRH in explicit form, which can be numerically evaluated.

3) We provide the closed-form power allocation solutions for two extremely important cases: 1) When the QoS exponent θ approaches zero, which corresponds to the conventional ergodic capacity maximization problem; 2) When the QoS exponent θ tends to infinity, which represents the strictly delay-limited case. We also extend our work to the more general multiuser case, where the optimal transmit power for each user is derived.

4) Our simulation results will show that the proposed algorithms significantly outperforms the existing algorithms. Additionally, by appropriately choosing the QoS exponent, our proposed delay-aware algorithm can guarantee a delay-outage probability below 10^{-9} , when the maximum tolerable end-to-end (E2E) delay is 1 ms, which satisfies the strict delay requirements of the future ultra-reliable low latency communications (URLLC).

The most closely related paper of our work is [11], where single transmitter is considered. The optimal power allocation can be readily derived in closed form by the aid of the Lagrangian dual decomposition, which is in the water-filling-like form. However, our considered C-RAN involves multiple independent transmitters, the power allocation derivations are much more involved, and the power allocation solution is not the same as the conventional water-filling form. In [11], only one dual variable needs to be optimized, which can be obtained by using the bisection search method, while multiple dual variables are involved in the C-RAN scenario and the subgradient method is adopted to update the dual variables. Furthermore, in both papers, the average power expression is required in the updating of dual variables. However, this issue is not studied in [11], while our paper provides more details about the analysis of this issue.

The rest of this paper is organized as follows. In Section II, the C-RAN system is introduced along with the concept of EC and our problem formulation. In Section III, we provide the optimal power allocation for the general case of any number of RRHs. In Section IV, we derive the integral expressions's closed-form solution concerning the average transmit power of each RRH for the sake of updating the Lagrangian dual variables. In Section V, we obtain the power allocation for two extreme cases, namely for the delay-tolerant scenario and

for extremely stringent delay constraints. Numerical results are also provided in Section VII. Finally, our conclusions are drawn in Section VIII. The other notations are summarized in Table. I.

II. SYSTEM MODEL

Consider a downlink C-RAN consisting of I RRHs and a single user¹, where each RRH and the user have a single antenna, as depicted in Fig. 1. The set of RRHs is denoted as $\mathcal{I} = \{1, 2, \dots, I\}$. All the RRHs are assumed to be connected to the BBU pool through the fronthaul links relying on high-speed fiber-optic cables. In Fig. 2, the upper layer packets are first buffered in first-in-first-out (FIFO) queue, which will be transmitted to the physical layer of the RRHs. Since the RRHs are only responsible for simple transmission/reception, we do not consider the storage function at the RRHs. At the data-link layer, the upper-layer packets are partitioned into frames and then each frame will be mapped into bit-streams at the physical layer. The channel is assumed to obey the stationary block fading model, implying that they are fixed during each time frame of length of T_f , while it is switched independently over different time frames.

To elaborate, we consider a Nakagami- m block-fading channel, which is very general and includes most of the practical wireless communication channels as special cases [17]. The parameter m represents the severeness of the channel, where the fading channel fluctuations are reduced with m . The probability density function (PDF) of the Nakagami- m channel spanning from the i -th RRH to the user is given by:

$$f(\alpha_i) = \frac{\alpha_i^{m-1}}{\Gamma(m)} \left(\frac{m}{\bar{\alpha}_i}\right)^m \exp\left(-\frac{m}{\bar{\alpha}_i}\alpha_i\right), \quad \alpha_i \geq 0, \quad (1)$$

where $\Gamma(m) = \int_0^\infty w^{m-1} e^{-w} dw$ is the Gamma function, α_i denotes the instantaneous channel-power-to-noise ratio (CPNR) from the i th RRH to the user, and $\bar{\alpha}_i$ is the average received CPNR at the user from the i th RRH, denoted as PL_i/σ^2 , where PL_i is the large-scale fading channel gain spanning from the i th RRH to the user that includes the path loss and shadowing effect, and σ^2 is the noise power.

Let us define $\alpha = [\alpha_1, \alpha_2, \dots, \alpha_I]^T$. Since $\alpha_1, \dots, \alpha_I$ are independent, the joint PDF of α is given by

$$f(\alpha) = f(\alpha_1)f(\alpha_2)\cdots f(\alpha_I). \quad (2)$$

A. Effective Capacity (EC)

This paper considers the E2E delay requirement for each packet. In C-RANs, the E2E delay, denoted as D_{\max} , includes the uplink (UL) and downlink (DL) transmission delays of D_T , queueing delay at the buffer of the BBU pool of D_q , and the fronthaul delay of D_F . Since the fronthaul links are usually deployed with high-speed fiber, the fronthaul delay is much less than 1 ms [18]. In addition, since the packet size in URLLC is very short, the UL and DL transmission can be finished within a very short time. Hence, the E2E delay is mainly dominated by the queueing delay at the buffer of the BBU pool, which is given by $D_q = D_{\max} - D_F - D_T$. In

¹The method developed in this paper can also be applied to the multi-user scenario, where all users apply the classical orthogonal frequency division multiplexing access (OFDMA) technique to remove the multi-user interference.

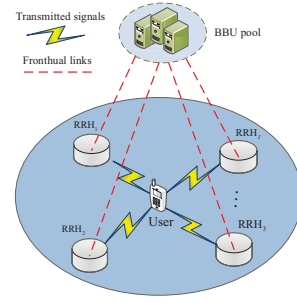


Fig. 1. Topology of a C-RAN with I RRHs.

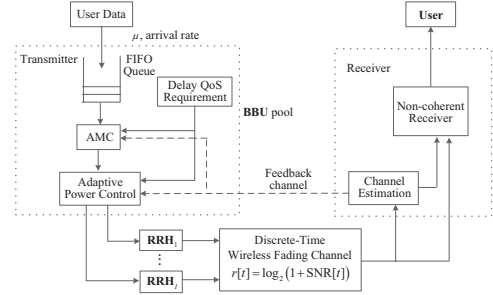


Fig. 2. Cross-layer transmission model.

the following, we mainly focus on the study of the queueing delay, which is characterized by the EC.

The EC is defined as the maximum constant frame arrival rate that a given service process can support, while obeying the delay requirement indicated by the QoS exponent θ that will be detailed later. Let the sequence $R[k], k = 1, 2, \dots$ represent the data service-rate, which follows a discrete-time stationary and ergodic stochastic process. The parameter k is the time frame index. Let us denote by $S(t) \triangleq \sum_{k=1}^t R[k]$ the partial sum of the service process over the time sequence spanning from $k = 1$ to $k = t$. Let us furthermore assume that the Gartner-Ellis limit of $S[t]$, which is denoted by $\Lambda_C(\theta) = \lim_{t \rightarrow \infty} (1/t) \log(\mathbb{E}\{e^{\theta S[t]}\})$, is a convex differentiable function for all real-value of θ [7]. Then, the EC of the service process specified by θ is

$$EC(\theta) = -\frac{\Lambda_C(-\theta)}{\theta} = -\frac{1}{\theta} \log(\mathbb{E}\{e^{-\theta R[k]}\}) \quad (3)$$

where $\mathbb{E}\{\cdot\}$ denotes the expectation operator.

Let us assume that a data source enters a queue of infinite buffer size at a constant data rate μ . The probability that the delay exceeds a maximum delay bound of D_q satisfies [6]

$$P_{\text{delay}}^{\text{out}} = \Pr\{\text{Delay} \geq D_q\} \approx \varepsilon e^{-\theta \mu D_q}, \quad (4)$$

where $f(x) \approx g(x)$ indicates that $\lim_{x \rightarrow \infty} [f(x)/g(x)] = 1$, and ε is the probability that the buffer is non-empty, which can be calculated by using the method in [6]. The parameter θ can be found by letting the constant arrival rate to be equal to the EC, i.e. setting it to $\mu = EC(\theta)$. Hence, if the delay-bound violation probability is required to be below $P_{\text{delay}}^{\text{out}}$, one should limit its incoming data rate to a maximum of $\mu = EC(\theta)$.

It is seen from (4) that θ is an important parameter, representing the decay rate of the delay violation probability. A smaller θ corresponds to a slower decay rate, which indicates that the delay requirement is loose, while a larger θ corresponds to a faster decay rate, which implies that the system

is capable of supporting a more stringent delay requirement. In other words, when $\theta \rightarrow 0$, an arbitrarily long delay can be tolerated by the system, which corresponds to the capacity studied in Shannon information theory. On the other hand, when $\theta \rightarrow \infty$, this implies that no delay is allowed by the system, which corresponds to the very stringent statistical delay-bound QoS constraint of allowing no delay at all.

B. Problem formulation

For the user, we assume that the non-coherent joint transmission is adopted as the BBU pool [19]–[21]. Then, the instantaneous service rate of a single frame, denoted by $R(\boldsymbol{\nu})$, can be expressed as follows [22], [23]:

$$R(\boldsymbol{\nu}) = T_f B \log_2(1 + \sum_{i \in \mathcal{I}} p_i(\boldsymbol{\nu}) \alpha_i), \quad (5)$$

where B is the system's bandwidth, $\boldsymbol{\nu} \triangleq (\boldsymbol{\alpha}, \theta)$ represents the network condition that includes both the channel's power gains and the EC exponent requirement, and $p_i(\boldsymbol{\nu})$ represents the power allocation for RRH i that depends on the network's condition $\boldsymbol{\nu}$. In this paper, we aim for optimizing the transmit power in order to maximize the EC for the user under two different types of power limitations for each RRH: under an average power constraint and a peak power constraint. The first one is related to the long-term power budget, while the second guarantees that the instantaneous transmit power is below the linear range of practical power amplifiers. Mathematically, this optimization problem can be formulated as

$$\max_{\{p_i(\boldsymbol{\nu}), i \in \mathcal{I}\}} -\frac{1}{\theta} \log \left(\mathbb{E}_{\boldsymbol{\alpha}} \left[e^{-\theta T_f B \log_2(1 + \sum_{i \in \mathcal{I}} p_i(\boldsymbol{\nu}) \alpha_i)} \right] \right) \quad (6a)$$

$$\text{s.t. } \mathbb{E}_{\boldsymbol{\alpha}} [p_i(\boldsymbol{\nu})] \leq P_i^{\text{avg}}, \forall i \in \mathcal{I}, \quad (6b)$$

$$0 \leq p_i(\boldsymbol{\nu}) \leq P_i^{\text{peak}}, \forall i \in \mathcal{I}, \quad (6c)$$

where $\mathbb{E}_{\boldsymbol{\alpha}}\{\cdot\}$ denotes the expectation over $\boldsymbol{\alpha}$, while P_i^{avg} and P_i^{peak} denote the i th RRH's maximum average transmit power constraint and peak transmit power constraint, respectively.

III. OPTIMAL POWER ALLOCATION METHOD

By exploiting the fact that $\log(\cdot)$ is a monotonically increasing function, Problem (6) can be equivalently simplified as

$$\min_{\{p_i(\boldsymbol{\nu}), \forall i \in \mathcal{I}\}} \mathbb{E}_{\boldsymbol{\alpha}} \left[\left(1 + \sum_{i \in \mathcal{I}} p_i(\boldsymbol{\nu}) \alpha_i \right)^{-\varepsilon(\theta)} \right] \quad (7a)$$

$$\text{s.t. } \mathbb{E}_{\boldsymbol{\alpha}} [p_i(\boldsymbol{\nu})] \leq P_i^{\text{avg}}, \forall i \in \mathcal{I}, \quad (7b)$$

$$0 \leq p_i(\boldsymbol{\nu}) \leq P_i^{\text{peak}}, \forall i \in \mathcal{I}, \quad (7c)$$

where we have $\varepsilon(\theta) = \theta T_f B / \ln 2$. In Appendix A of our longer version paper [24], we prove that Problem (7) is a convex optimization problem. Hence, the Lagrangian duality method can be used to solve Problem (7) with zero optimality gap.

Note that in Problem (7), only the average power constraints are ergodic, while the others are instantaneous power constraints. Similar to [25], we should first introduce the dual variables associated with the average transmit power constraints. Then, the original problem can be decomposed into several independent subproblems, where each one corresponds to one fading state. In addition, the instantaneous power constraints are enforced for each fading state. Let $\boldsymbol{\lambda} = [\lambda_1, \dots, \lambda_I]^T$ represent the nonnegative dual variables

associated with the average power constraints. The Lagrangian function of Problem (7) can be written as

$$\begin{aligned} \mathcal{L}(\mathbf{P}(\boldsymbol{\nu}), \boldsymbol{\lambda}) &= \mathbb{E}_{\boldsymbol{\alpha}} \left[(1 + \sum_{i \in \mathcal{I}} p_i(\boldsymbol{\nu}) \alpha_i)^{-\varepsilon(\theta)} \right] \\ &+ \sum_{i \in \mathcal{I}} \lambda_i (\mathbb{E}_{\boldsymbol{\alpha}} [p_i(\boldsymbol{\nu})] - P_i^{\text{avg}}), \end{aligned} \quad (8)$$

where $\mathbf{P}(\boldsymbol{\nu}) = [p_1(\boldsymbol{\nu}), \dots, p_I(\boldsymbol{\nu})]^T$. Let us now define $\mathcal{P} = \{\mathbf{P}(\boldsymbol{\nu}) | (7c)\}$. The Lagrange dual function is then given by

$$g(\boldsymbol{\lambda}) = \min_{\mathbf{P}(\boldsymbol{\nu}) \in \mathcal{P}} \mathcal{L}(\mathbf{P}(\boldsymbol{\nu}), \boldsymbol{\lambda}). \quad (9)$$

The dual problem is defined as

$$\max_{\lambda_i \geq 0, \forall i} g(\boldsymbol{\lambda}). \quad (10)$$

As proven in Appendix A of [24], Problem (7) is a convex optimization problem, which implies that there is no duality gap between the dual problem and the original problem. Thus, solving the dual problem is equivalent to solving the original problem.

To solve the dual problem in (10), we should solve the problem in (9) for a fixed $\boldsymbol{\lambda}$, then update the Lagrangian dual variables $\boldsymbol{\lambda}$ by solving the dual problem in (10). Iterate the above two steps until convergence is reached.

1) *Solving the dual function in (9)*: For a given $\boldsymbol{\lambda}$, we should find the dual function $g(\boldsymbol{\lambda})$, which can be rewritten as

$$g(\boldsymbol{\lambda}) = \mathbb{E} [\tilde{g}(\boldsymbol{\lambda})] - \sum_{i \in \mathcal{I}} \lambda_i P_i^{\text{avg}}, \quad (11)$$

where we have:

$$\tilde{g}(\boldsymbol{\lambda}) = \min_{\mathbf{P}(\boldsymbol{\nu}) \in \mathcal{P}} \left(1 + \sum_{i \in \mathcal{I}} p_i(\boldsymbol{\nu}) \alpha_i \right)^{-\varepsilon(\theta)} + \sum_{i \in \mathcal{I}} \lambda_i p_i(\boldsymbol{\nu}). \quad (12)$$

Note that $\tilde{g}(\boldsymbol{\lambda})$ can be decoupled into multiple independent subproblems, each corresponding to a specific fading state. Those subproblems have the same structure for each fading state. Hence, to simplify the derivation, $\boldsymbol{\nu}$ is omitted in the following. Each subproblem can be expressed as:

$$\min_{\mathbf{P}} \left(1 + \sum_{i \in \mathcal{I}} p_i \alpha_i \right)^{-\varepsilon(\theta)} + \sum_{i \in \mathcal{I}} \lambda_i p_i \quad (13a)$$

$$\text{s.t. } 0 \leq p_i \leq P_i^{\text{peak}}, \forall i \in \mathcal{I}. \quad (13b)$$

The above problem is convex. In the following, we obtain the closed-form solution by solving the KKT conditions of Problem (13).

First, we introduce the nonnegative dual variables of $\mu_i, \forall i$, and $\delta_i, \forall i$ for the associated constraints in (13b). The KKT conditions for Problem (13) can be expressed as

$$-\varepsilon(\theta) \left(1 + \sum_{i \in \mathcal{I}} p_i^* \alpha_i \right)^{-\varepsilon(\theta)-1} \alpha_i + \lambda_i + \mu_i^* - \delta_i^* = 0, \forall i \quad (14a)$$

$$\mu_i^* (p_i^* - P_i^{\text{peak}}) = 0, \forall i \quad (14b)$$

$$\delta_i^* p_i^* = 0, \forall i \quad (14c)$$

$$p_i^* \leq P_i^{\text{peak}}, \forall i \quad (14d)$$

$$p_i^* \geq 0, \forall i, \quad (14e)$$

with $p_i^* \geq 0$, $\delta_i^* \geq 0$, and $\mu_i^* \geq 0$, $\forall i$. Then, we have the following lemma.

Lemma 1: For any two arbitrary RRHs i and j , if $p_i^* > 0$ and $p_j^* = 0$, then the following relationship must hold

$$\frac{\lambda_i}{\alpha_i} \leq \frac{\lambda_j}{\alpha_j}. \quad (15)$$

Proof: Please see Appendix B of [24]. ■

Lemma 1 shows that the RRHs associated with a smaller λ_i/α_i should be assigned a non-zero power, while the RRHs having a larger value should remain silent. Let us hence introduce π as a permutation over \mathcal{I} , so that we have $\frac{\lambda_{\pi(i)}}{\alpha_{\pi(i)}} \leq \frac{\lambda_{\pi(j)}}{\alpha_{\pi(j)}}$, when $i < j, i, j \in \mathcal{I}$. Let $\mathcal{I}' \subseteq \mathcal{I}$ be the set of RRHs that transmit at a non-zero power. Then, according to Lemma 1, it can be readily verified that we have $\mathcal{I}' = \{\pi(1), \dots, \pi(|\mathcal{I}'|)\}$.

Lemma 2: There is at most one RRH associated with $0 < p_i^* < P_i^{\text{peak}}$, and the RRH index is $i = \pi(|\mathcal{I}'|)$.

Proof: Please see Appendix C of [24]. ■

Next, we derive the optimal power allocation of Problem (13) shown as in Theorem 1.

Theorem 1: The optimal solution of Problem (13) is shown as follows,

$$P_{\pi(a)}^* = \begin{cases} P_{\pi(a)}^{\text{peak}}, & a < |\mathcal{I}'|; \\ \min \left\{ P_{\pi(|\mathcal{I}'|)}^{\text{peak}}, T_{\pi(a)} \right\}, & a = |\mathcal{I}'|; \\ 0, & a > |\mathcal{I}'|; \end{cases} \quad (16)$$

where $T_{\pi(a)}$ is given by

$$T_{\pi(a)} = \frac{1}{\alpha_{\pi(|\mathcal{I}'|)}} \left[\left(\frac{\lambda_{\pi(|\mathcal{I}'|)}}{\varepsilon(\theta)\alpha_{\pi(|\mathcal{I}'|)}} \right)^{-\frac{1}{\varepsilon(\theta)+1}} - \sum_{a=1}^{|\mathcal{I}'|-1} P_{\pi(a)}^{\text{peak}} \alpha_{\pi(a)} - 1 \right]$$

with $|\mathcal{I}'|$ being the largest value of integer x , so that we have

$$\frac{\lambda_{\pi(x)}}{\varepsilon(\theta)\alpha_{\pi(x)}} < \left[\sum_{b=1}^{x-1} P_{\pi(b)}^{\text{peak}} \alpha_{\pi(b)} + 1 \right]^{-\varepsilon(\theta)-1}. \quad (17)$$

Proof: Please refer to Appendix D of [24]. ■

It can be seen from (16) that the RRHs with high value of λ_i/α_i should be switched off, and the ones with larger values can transmit with peak power. The dual variable λ_i can be regarded as the price, and larger value of λ_i will incur higher cost when the RRH is active.

Corollary 1: When the number of RRHs is equal to one, i.e. $I = 1$, the optimal transmit power is given by

$$p_1^* = \begin{cases} 0, & \text{if } \alpha_1 < \frac{\lambda_1}{\varepsilon(\theta)}; \\ F, & \text{if } \alpha_1 \geq \frac{\lambda_1}{\varepsilon(\theta)} \text{ and } F < P_1^{\text{peak}}; \\ P_1^{\text{peak}}, & \text{if } \alpha_1 \geq \frac{\lambda_1}{\varepsilon(\theta)} \text{ and } F \geq P_1^{\text{peak}}. \end{cases} \quad (18)$$

where F is given by

$$F = \frac{1}{(\lambda_1/\varepsilon(\theta))^{1/1+\varepsilon(\theta)} \alpha_1^{\varepsilon(\theta)/1+\varepsilon(\theta)}} - \frac{1}{\alpha_1}.$$

Proof: It is can be readily derived using Theorem 1. ■

Note that the above result is consistent with the point-to-point result obtained in [11].

2) *Solving the dual problem (10):* To solve the dual problem (10), we invoke the subgradient method, which is a simple method of optimizing non-differentiable objective function [26]. The subgradient is required by the subgradient of $g(\cdot)$ at $\lambda^{(k)} = [\lambda_1^{(k)}, \dots, \lambda_I^{(k)}]^T$ in the k th iteration².

Theorem 2: The subgradient of $g(\cdot)$ at $\lambda^{(k)}$ in the k th iteration is given by

$$\mathbf{d}^{(k)} = \mathbb{E}_{\boldsymbol{\nu}} \left[\mathbf{P}_{\lambda^{(k)}}^* (\boldsymbol{\nu}) \right] - \mathbf{P}^{\text{avg}}, \quad (19)$$

where $\mathbf{P}_{\lambda^{(k)}}^* (\boldsymbol{\nu}) = \left[p_{(1, \lambda^{(k)})}^* (\boldsymbol{\nu}), \dots, p_{(I, \lambda^{(k)})}^* (\boldsymbol{\nu}) \right]^T$ is the opti-

²According to [26], a vector \mathbf{d} is a subgradient of $g(\lambda)$ at $\lambda^{(k)}$, if for all λ , $g(\lambda) \leq g(\lambda^{(k)}) + \mathbf{d}^T (\lambda - \lambda^{(k)})$ holds.

mal solution of Problem (9) when we have $\lambda = \lambda^{(k)}$, and $\mathbf{P}^{\text{avg}} = [P_1^{\text{avg}}, \dots, P_I^{\text{avg}}]^T$.

Proof: Please see Appendix E of [24]. ■

Based on Theorem 2, the Lagrangian dual variables can be updated as

$$\lambda^{(k+1)} = \lambda^{(k)} + \zeta^{(k)} \mathbf{d}^{(k)}, \quad (20)$$

where $\zeta^{(k)}$ is the step in the k th iteration. The subgradient method is guaranteed to converge if $\zeta^{(k)}$ satisfies $\lim_{k \rightarrow \infty} \zeta^{(k)} = 0$ and $\sum_{k=1}^{\infty} \zeta^{(k)} = \infty$ [27]. The step size in the simulation section is set as $\zeta^{(k)} = a/k$, where a is the constant step-size parameter.

In summary, the solution of Problem (6) is given in Algorithm 1. To execute Algorithm 1, there is another issue

Algorithm 1 Solving Problem (6)

Initialize:

Iteration number $k = 0$, $\lambda^{(0)} = [\lambda_1^{(0)}, \dots, \lambda_I^{(0)}]$;

Repeat

1. Compute $\mathbf{P}^{(k)}$ with fixed $\lambda^{(k)}$ using (16);

2. Compute the subgradient $\mathbf{d}^{(k)}$, using (19);

3. Update $\lambda^{(k+1)}$ using (20), increase k by 1;

Until convergence

that has to be tackled, namely how to calculate the average power for each RRH in order to obtain the subgradient $\mathbf{d}^{(k)}$. Given the dual variables $\lambda^{(k)}$, the expression of optimal power at each RRH depends on the generations of channel gains α . Different generations of α will lead to different orders of $\lambda_i/\alpha_i, i = 1, \dots, I$, and thus different power expressions. Even for a fixed problem-order the power allocation expressions require multiple integrations, which imposes a high computational complexity. As a result, it is a challenge to obtain the expression of average power for each RRH in closed-form for any given $\lambda^{(k)}$. In fact, even for the simple case of two RRHs, the average powers generally do not have simple closed-form solutions, as shown in the next section.

To resolve the above issue, we propose an online calculation method for tracking the average power required for each RRH. The main idea is to replace the expectation operator by averaging the power allocations for all samples of channel generations during the fading process. Specifically, let us define $\bar{P}_i^{(k-1)}$ as

$$\bar{P}_i^{(k-1)} = \frac{1}{k-1} \sum_{j=1}^{k-1} p_{(i, \lambda^{(j)})}^* (\boldsymbol{\alpha}^{(j)}, \theta), i = 1, \dots, I, \quad (21)$$

where $p_{(i, \lambda^{(j)})}^* (\boldsymbol{\alpha}^{(j)}, \theta)$ denotes the optimal power allocation of the i th RRH for the j th channel generation, and $\lambda^{(j)}$ represents the corresponding dual variables. Then, the expectation over $p_{(i, \lambda^{(k)})}^* (\boldsymbol{\nu})$ can be approximated as

$$\mathbb{E}_{\boldsymbol{\nu}} \left[p_{(i, \lambda^{(k)})}^* (\boldsymbol{\nu}) \right] \approx \bar{P}_i^{(k)} = \frac{p_{(i, \lambda^{(k)})}^* (\boldsymbol{\alpha}^{(k)}, \theta) + (k-1) \bar{P}_i^{(k-1)}}{k}, \forall i \in \mathcal{I}, \quad (22)$$

which can be recursively obtained based on the previous $\bar{P}_i^{(k-1)}, \forall i$. It is worth noting that this algorithm can be readily applied to the case when the fading statistics are unknown.

Fortunately, for the case of a single RRH³, the average

³Note that [11] did not provide the closed-form expression for the average power for the case of one RRH.

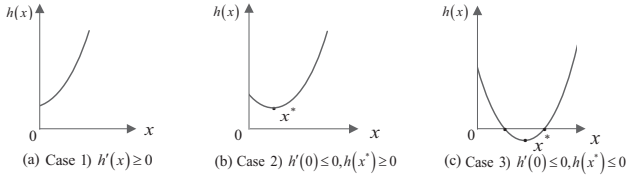


Fig. 3. The properties of the function $h(x) = (1+ax)^b - cx$. power can be obtained in closed-form, which is given in Appendix F of [24]. The average power expression for the case of $I = 2$ is even more complex, which is extensively studied in the following section.

IV. SPECIAL CASE: $I = 2$

To show the difficulty of obtaining the closed-form solution for each RRH, we only consider the simplest scenario of two RRHs, i.e., $I = 2$. To this end, we first introduce the following lemma, which will be used in the ensuing derivations.

Lemma 3: Let us define the function $h(x) = (1+ax)^b - cx$, where $a > 0, c > 0, b > 1$. Then, when $x \geq 0$, there are only three possible curves for the function $h(x)$, which are shown in Fig. 3. The conditions for each case are given as follows:

- 1) Case 1: $ab - c \geq 0$;
- 2) Case 2: $ab - c < 0$ and $(\frac{c}{ab})^{1/(b-1)}(1-b) + b \geq 0$;
- 3) Case 3: $ab - c < 0$ and $(\frac{c}{ab})^{1/(b-1)}(1-b) + b < 0$;

Proof: Please see Appendix G of [24]. ■

Based on Lemma 3, we commence by deriving the expression of the average transmit power. According to Theorem 1, there are three different possible cases for $I = 2$: 1) $|\mathcal{I}'| = 0$; 2) $|\mathcal{I}'| = 1$; 3) $|\mathcal{I}'| = 2$. Obviously, the average power contributed by the first case is zero, hence we only consider the latter two cases, which are discussed in the next two subsections. Without loss of generality, we assume that

$$\frac{\lambda_1}{\alpha_1} \leq \frac{\lambda_2}{\alpha_2} \quad (23)$$

holds. The case for $\frac{\lambda_1}{\alpha_1} > \frac{\lambda_2}{\alpha_2}$ can be similarly derived.

A. Scenario 1: There is only one RRH that transmits at a non-zero power, i.e., $|\mathcal{I}'| = 1$

Since we have assumed that the inequality (23) holds, only RRH 1 is transmitting at a non-zero power and RRH 2 remains silent in this case. According to Theorem 1, the conditions for $|\mathcal{I}'| = 1$ are given by

$$\frac{\lambda_2}{\varepsilon(\theta)\alpha_2} \geq \left(P_1^{\text{peak}}\alpha_1 + 1\right)^{-\varepsilon(\theta)-1}, \quad (24)$$

$$\frac{\lambda_1}{\varepsilon(\theta)\alpha_1} < 1, \quad (25)$$

and only RRH 1 transmits non-zero power, which is given by

$$p_1^* = \min \left\{ P_1^{\text{peak}}, \frac{1}{\alpha_1} \left[\left(\frac{\lambda_1}{\varepsilon(\theta)\alpha_1} \right)^{-\frac{1}{\varepsilon(\theta)+1}} - 1 \right] \right\}. \quad (26)$$

It may be readily seen that, there are two possible values of p_1^* , and the conditions for each value will be discussed as follows.

1) $p_1^* = P_1^{\text{peak}}$: In this case, the following condition should be satisfied:

$$\frac{1}{\alpha_1} \left[\left(\frac{\lambda_1}{\varepsilon(\theta)\alpha_1} \right)^{-\frac{1}{\varepsilon(\theta)+1}} - 1 \right] \geq P_1^{\text{peak}}, \quad (27)$$

which is equivalent to

$$\left(1 + P_1^{\text{peak}}\alpha_1\right)^{1+\varepsilon(\theta)} - \frac{\varepsilon(\theta)}{\lambda_1}\alpha_1 \leq 0. \quad (28)$$

Notice that the left hand side of (28) is in the form of $h(x)$ defined in Lemma 3, with $x = \alpha_1, a, b, c$ given by

$$a = P_1^{\text{peak}}, b = 1 + \varepsilon(\theta), c = \varepsilon(\theta)/\lambda_1. \quad (29)$$

To guarantee that there exists a positive α_1 , the function $h(x)$ should be reminiscent of Fig. 3-(c), and the conditions for Case 3 in Lemma 3 should be satisfied. Otherwise, p_1^* is not equal to P_1^{peak} . In the following, we assume that the conditions are satisfied. Let us denote the solutions of $h(\alpha_1) = 0$ as α_1^l and α_1^u , where $\alpha_1^l < \alpha_1^u$. These solutions can be readily obtained by using the classic bisection method. Then, condition (28) is equivalent to

$$\alpha_1^l \leq \alpha_1 \leq \alpha_1^u. \quad (30)$$

By combining (23) and (24), we obtain the feasible region of α_2 in the form of:

$$\begin{aligned} 0 \leq \alpha_2 &\leq \min \left(\frac{\lambda_2}{\lambda_1}\alpha_1, \frac{\lambda_2}{\varepsilon(\theta)} \left(1 + P_1^{\text{peak}}\alpha_1\right)^{1+\varepsilon(\theta)} \right) \\ &= \frac{\lambda_2}{\varepsilon(\theta)} \left(1 + P_1^{\text{peak}}\alpha_1\right)^{1+\varepsilon(\theta)}, \end{aligned} \quad (31)$$

where the last equality holds by using (28). Similarly, by combining (25) and (30), we obtain the feasible region of α_1 as:

$$\max \left(\alpha_1^l, \frac{\lambda_1}{\varepsilon(\theta)} \right) \leq \alpha_1 \leq \alpha_1^u. \quad (32)$$

In this context, we prove that $\lambda_1/\varepsilon(\theta) < \alpha_1^l$ in Appendix H of [24]. Hence, the feasible region of α_1 is given by $\alpha_1^l \leq \alpha_1 \leq \alpha_1^u$.

Based on the above discussions, we obtain the conditions for $p_1^* = P_1^{\text{peak}}, p_2^* = 0$ as follows:

$$\text{C1} : ab - c < 0, \left(\frac{c}{ab}\right)^{1/(b-1)}(1-b) + b < 0, \quad (33)$$

where a, b, c are given in (29).

If Condition C1 in (33) is satisfied, the average power assigned to RRH 1 in this case is given by

$$T_{\text{RRH1}}^{\text{C1}} \triangleq \int_{\alpha_1^l}^{\alpha_1^u} \int_0^{\frac{\lambda_2}{\varepsilon(\theta)}(1+P_1^{\text{peak}}\alpha_1)^{1+\varepsilon(\theta)}} P_1^{\text{peak}} f(\alpha_1) f(\alpha_2) d\alpha_2 d\alpha_1. \quad (34)$$

By substituting the PDF of α_2 in (2) into (34), (34) can be simplified to

$$\begin{aligned} T_{\text{RRH1}}^{\text{C1}} &= \\ &\frac{P_1^{\text{peak}}}{\Gamma(m)} \int_{\alpha_1^l}^{\alpha_1^u} f(\alpha_1) \gamma \left(m, \frac{m\lambda_2}{\alpha_2\varepsilon(\theta)} \left(1 + P_1^{\text{peak}}\alpha_1\right)^{1+\varepsilon(\theta)} \right) d\alpha_1. \end{aligned} \quad (35)$$

Unfortunately, the closed-form expression of $T_{\text{RRH1}}^{\text{C1}}$ cannot be obtained even for the special case of $m = 1$. However, the value of $T_{\text{RRH1}}^{\text{C1}}$ can be obtained at a good accuracy by using the numerical integration function of Matlab.

2) $p_1^* = \frac{1}{\alpha_1} \left[\left(\frac{\lambda_1}{\varepsilon(\theta)\alpha_1} \right)^{-\frac{1}{\varepsilon(\theta)+1}} - 1 \right]$: In this case, the following condition should be satisfied:

$$\frac{1}{\alpha_1} \left[\left(\frac{\lambda_1}{\varepsilon(\theta)\alpha_1} \right)^{-\frac{1}{\varepsilon(\theta)+1}} - 1 \right] < P_1^{\text{peak}}, \quad (36)$$

which leads to $h(\alpha_1) > 0$ with a, b, c defined in (29). As seen from Fig. 3, when the first two conditions in Lemma 3 are

satisfied, the inequality (36) holds for any $\alpha_1 \geq 0$. When the third condition in Lemma 3 is satisfied, the inequality (36) holds when $0 \leq \alpha_1 \leq \alpha_1^l$ and $\alpha_1 \geq \alpha_1^u$, where α_1^l and α_1^u ($\alpha_1^l < \alpha_1^u$) are the solutions of $h(\alpha_1) = 0$ with a, b, c defined in (29).

Now, we first assume that the first two conditions in Lemma 3 are satisfied

$$\text{C2: } ab - c \geq 0, \text{ or } ab - c < 0 \text{ and } \left(\frac{c}{ab}\right)^{\frac{1}{1-b}}(1-b) + b \geq 0 \quad (37)$$

where a, b, c are given in (29). Then, the condition in (36) can be neglected. According to (23) and (24), the feasible region of α_2 is given by

$$0 \leq \alpha_2 \leq \min\left(\frac{\lambda_2}{\lambda_1} \alpha_1, \frac{\lambda_2}{\varepsilon(\theta)} \left(1 + P_1^{\text{peak}} \alpha_1\right)^{1+\varepsilon(\theta)}\right) = \frac{\lambda_2}{\lambda_1} \alpha_1, \quad (38)$$

where (36) is used in the last equality. From (25), the feasible region of α_1 is given by $\alpha_1 \geq \frac{\lambda_1}{\varepsilon(\theta)}$. As a result, the average power of RRH 1 contributed by the case when condition C2 is satisfied is given by

$$\begin{aligned} T_{\text{RRH1}}^{\text{C2}} &= \int_{\frac{\lambda_1}{\varepsilon(\theta)}}^{\infty} \int_0^{\frac{\lambda_2}{\lambda_1} \alpha_1} p_1^* f(\alpha_1) f(\alpha_2) d\alpha_2 d\alpha_1, \\ &= \frac{1}{\Gamma(m)} \int_{\frac{\lambda_1}{\varepsilon(\theta)}}^{\infty} p_1^* \gamma\left(m, \frac{m\lambda_2 \alpha_1}{\alpha_2 \lambda_1}\right) f(\alpha_1) d\alpha_1. \end{aligned} \quad (39)$$

Fortunately, when m is an integer, the closed-form expression of $T_{\text{RRH1}}^{\text{C2}}$ can be obtained. Let us define

$$\begin{aligned} U &\triangleq \frac{\lambda_1}{\varepsilon(\theta)}, V \triangleq \frac{1}{1+\varepsilon(\theta)}, W \triangleq \frac{m\lambda_2}{\alpha_2 \lambda_1}, \\ Z &\triangleq \frac{(m/\alpha_1)^m}{(m-1)!}, Y \triangleq \frac{m\lambda_2}{\alpha_2 \lambda_1} + \frac{m}{\alpha_1}. \end{aligned} \quad (40)$$

If $m = 1$, the Nakagami- m channel reduces to the Rayleigh channel, and the average power of RRH 1 in (39) can be simplified to:

$$\begin{aligned} T_{\text{RRH1}}^{\text{C2}} &= \frac{\alpha_1^{V-1} \Gamma(V, U/\alpha_1)}{U^V} + \frac{1}{\alpha_1} \text{Ei}\left(-\frac{U}{\alpha_1}\right) \\ &\quad - \frac{\Gamma(V, UY)}{\alpha_1 Y^V U^V} - \frac{1}{\alpha_1} \text{Ei}(-UY). \end{aligned} \quad (41)$$

If m is an integer that is larger than one, i.e., $m \geq 2$, we can obtain the closed-form expression of $T_{\text{RRH1}}^{\text{C2}}$:

$$T_{\text{RRH1}}^{\text{C2}} = J_1 + J_2 - J_3 - J_4, \quad (42)$$

where J_1, J_2, J_3 and J_4 are respectively given by

$$\begin{aligned} J_1 &= \frac{\alpha_1^{V-1} \Gamma(V+m-1, \frac{mU}{\alpha_1})}{(m-1)! m^{V-1} U^V}, \\ J_2 &= Z \sum_{l=0}^{m-1} \frac{W^l}{l! Y^{l+m-1}} \Gamma(l+m-1, YU), \\ J_3 &= \frac{Z}{U^V} \sum_{l=0}^{m-1} \frac{W^l}{l! Y^{l+V+m-1}} \Gamma(l+V+m-1, YU), \\ J_4 &= \frac{m}{\alpha_1(m-1)!} \Gamma\left(m-1, \frac{mU}{\alpha_1}\right). \end{aligned} \quad (43)$$

The details of derivations can be found in Appendix I of [24].

Next, we consider the case, where Condition 3) in Lemma 3 is satisfied. According to the condition in (36), the feasible region of α_1 is $0 \leq \alpha_1 \leq \alpha_1^l$ and $\alpha_1 \geq \alpha_1^u$. Additionally, from (25), $\alpha_1 \geq U$ should hold. According to Appendix H of [24], $U \leq \alpha_1^l$ always holds. Hence, the overall feasible region is $\alpha_1^l \geq \alpha_1 \geq U$ and $\alpha_1 \geq \alpha_1^u$. Furthermore, the feasible region of α_2 is the same as in (38). As a result, the

expression of the average power for RRH 1 contributed in this case can be similarly obtained as in (39), except for the different integration intervals for α_1 . The expression for the special case, when m is an integer can be similarly obtained.

Let us now define the following function

$$F(x) = \frac{1}{\Gamma(m)} \int_x^{\infty} \frac{1}{\alpha_1} \left[\left(\frac{\alpha_1}{U}\right)^V - 1 \right] \gamma(m, W\alpha_1) f(\alpha_1) d\alpha_1.$$

Then, $T_{\text{RRH1}}^{\text{C2}}$ given in (39) is equal to $T_{\text{RRH1}}^{\text{C2}} = F(U)$.

If the following condition is satisfied:

$$\text{C3: } ab - c < 0 \text{ and } \left(\frac{c}{ab}\right)^{1/(b-1)}(1-b) + b < 0, \quad (45)$$

with a, b, c given in (29), the average power for RRH 1 contributed under this condition is

$$T_{\text{RRH1}}^{\text{C3}} = F(U) - F(\alpha_1^l) + F(\alpha_1^u). \quad (46)$$

Note that Condition C3 is the same as Condition C1, but the power allocation for RRH 1 is different.

B. Scenario 2: Both RRHs are transmitting at a non-zero power, i.e., $|\mathcal{I}'| = 2$

In this case, RRH 1 will transmit with full power, i.e., $p_1^* = P_1^{\text{peak}}$, and RRH 2 will transmit at a non-zero power. According to Theorem 1, the following condition should be satisfied:

$$\frac{\lambda_2}{\varepsilon(\theta) \alpha_2} < \left(1 + P_1^{\text{peak}} \alpha_1\right)^{-\varepsilon(\theta)-1} \quad (47)$$

and the transmit power of RRH 2 is given by

$$p_2^* = \min\left\{P_2^{\text{peak}}, \frac{1}{\alpha_2} \left[\left(\frac{\lambda_2}{\varepsilon(\theta) \alpha_2}\right)^{-\frac{1}{1+\varepsilon(\theta)}} - P_1^{\text{peak}} \alpha_1 - 1 \right]\right\}. \quad (48)$$

The conditions for each value of p_2^* will be discussed as follows.

1) $p_2^* = P_2^{\text{peak}}$: In this case, the following condition should be satisfied:

$$P_2^{\text{peak}} \leq \frac{1}{\alpha_2} \left[\left(\frac{\lambda_2}{\varepsilon(\theta) \alpha_2}\right)^{-\frac{1}{1+\varepsilon(\theta)}} - P_1^{\text{peak}} \alpha_1 - 1 \right]. \quad (49)$$

Combining conditions (23), (47) and (49), we can obtain the feasible region of α_1 as follows

$$\frac{\lambda_1}{\lambda_2} \alpha_2 \leq \alpha_1 < \frac{1}{P_1^{\text{peak}}} \left[\left(\frac{\varepsilon(\theta) \alpha_2}{\lambda_2}\right)^{\frac{1}{1+\varepsilon(\theta)}} - P_2^{\text{peak}} \alpha_2 - 1 \right] \triangleq A. \quad (50)$$

To guarantee that we have a nonempty set of α_1 , the following condition should be satisfied:

$$\left(1 + P_2^{\text{peak}} \alpha_2 + \frac{\lambda_1}{\lambda_2} P_1^{\text{peak}} \alpha_2\right)^{1+\varepsilon(\theta)} < \frac{\varepsilon(\theta)}{\lambda_2} \alpha_2, \quad (51)$$

which is in the form of function $h(x)$ defined in Lemma 3 with $x = \alpha_2$, and a, b, c given by

$$a = P_2^{\text{peak}} + \frac{\lambda_1}{\lambda_2} P_1^{\text{peak}}, b = 1 + \varepsilon(\theta), c = \frac{\varepsilon(\theta)}{\lambda_2}. \quad (52)$$

To guarantee the existence of a positive α_2 , the graphical curve of the function $h(\alpha_2)$ should be similar to that in Fig. 3-c, and the conditions are given by

$$\text{C4: } ab - c < 0, \text{ and } \left(\frac{c}{ab}\right)^{1/(b-1)}(1-b) + b < 0, \quad (53)$$

where a, b, c are given in (52). Let us denote the solutions of $h(\alpha_2) = 0$ as α_2^l and α_2^u , where we have $\alpha_2^l < \alpha_2^u$. Then, the feasible region of α_2 is given by $\alpha_2^l < \alpha_2 < \alpha_2^u$.

Under Condition C4, the average powers of RRH 1 and RRH 2 are respectively calculated as

$$T_{\text{RRH1}}^{\text{C4}} = \frac{P_1^{\text{peak}}}{\Gamma(m)} \int_{\alpha_2^l}^{\alpha_2^u} f(\alpha_2) \left[\gamma\left(m, \frac{mA}{\bar{\alpha}_1}\right) - \gamma\left(m, \frac{m\lambda_1 \alpha_2}{\bar{\alpha}_1 \lambda_2}\right) \right] d\alpha_2, \quad (54)$$

$$T_{\text{RRH2}}^{\text{C4}} = \frac{T_{\text{RRH1}}^{\text{C4}} P_2^{\text{peak}}}{P_1^{\text{peak}}}, \quad (55)$$

where A is defined in (50).

2) $p_2^* = \frac{1}{\alpha_2} \left[\left(\frac{\lambda_2}{\varepsilon(\theta) \alpha_2} \right)^{-\frac{1}{1+\varepsilon(\theta)}} - P_1^{\text{peak}} \alpha_1 - 1 \right]$: In this case, the following condition should be satisfied:

$$P_2^{\text{peak}} > \frac{1}{\alpha_2} \left[\left(\frac{\lambda_2}{\varepsilon(\theta) \alpha_2} \right)^{-\frac{1}{1+\varepsilon(\theta)}} - P_1^{\text{peak}} \alpha_1 - 1 \right]. \quad (56)$$

By combining (23), (47) and (56), the feasible region of α_1 can be obtained as follows:

$$B \triangleq \frac{1}{P_1^{\text{peak}}} \left[\left(\frac{\varepsilon(\theta) \alpha_2}{\lambda_2} \right)^{\frac{1}{1+\varepsilon(\theta)}} - 1 \right] > \alpha_1 \geq \max \left\{ \frac{\lambda_1}{\lambda_2} \alpha_2, A \right\}, \quad (57)$$

where A is defined in (50). Note that $B > A$ always holds. Hence, to guarantee that there exists a feasible α_1 , the following condition should be satisfied:

$$0 \geq \left(1 + \frac{\lambda_1}{\lambda_2} P_1^{\text{peak}} \alpha_2 \right)^{1+\varepsilon(\theta)} - \frac{\varepsilon(\theta) \alpha_2}{\lambda_2}. \quad (58)$$

Again, the right hand side of (58) is in the form of the function $h(x)$ defined in Lemma 3, with $x = \alpha_2$, and a, b, c are given by

$$a = \frac{\lambda_1}{\lambda_2} P_1^{\text{peak}}, b = 1 + \varepsilon(\theta), c = \frac{\varepsilon(\theta)}{\lambda_2}. \quad (59)$$

To guarantee that there exists a positive α_2 , the third condition in Lemma 3 should be satisfied:

$$C_X : ab - c < 0 \text{ and } \left(\frac{c}{ab} \right)^{1/(b-1)} (1-b) + b < 0, \quad (60)$$

where a, b, c are given in (59). When a, b, c are given in (59), we can denote the solutions of $h(\alpha_2) = 0$ as $\tilde{\alpha}_2^l$ and $\tilde{\alpha}_2^u$ with $\tilde{\alpha}_2^l < \tilde{\alpha}_2^u$. Hence, the feasible region of α_2 is given by $\tilde{\alpha}_2^l < \alpha_2 < \tilde{\alpha}_2^u$.

The remaining task is to determine the lower bound of α_1 as shown in (57).

Case I: If the following condition is satisfied:

$$\frac{\lambda_1}{\lambda_2} \alpha_2 \geq A, \quad (61)$$

the feasible region of α_1 is given by

$$B > \alpha_1 \geq \frac{\lambda_1}{\lambda_2} \alpha_2, \quad (62)$$

where B is defined in (57). The inequality (61) can be rewritten as

$$\left(1 + P_2^{\text{peak}} \alpha_2 + \frac{\lambda_1 P_1^{\text{peak}}}{\lambda_2} \alpha_2 \right)^{1+\varepsilon(\theta)} \geq \frac{\varepsilon(\theta) \alpha_2}{\lambda_2}, \quad (63)$$

which is equivalent to $h(\alpha_2) \geq 0$ with a, b and c given in (52).

As seen from Fig. 3, when the first two conditions in Lemma 3 are satisfied, the inequality (63) holds for any $\alpha_2 > 0$. Combining this with the condition (58), the feasible region of α_2 is given by $\tilde{\alpha}_2^l < \alpha_2 < \tilde{\alpha}_2^u$, where $\tilde{\alpha}_2^l$ and $\tilde{\alpha}_2^u$ are the solutions of $h(\alpha_2) = 0$ with a, b, c defined in (59). Define the following condition with a, b, c defined in (52)⁴:

$$C5 : C_X \text{ and } ab - c \geq 0, \text{ or } C_X, ab - c < 0 \text{ and } \left(\frac{c}{ab} \right)^{1/(b-1)} (1-b) + b \geq 0, \quad (64)$$

and C_X as

$$C_X \triangleq \frac{1}{\alpha_2} \left[\left(\frac{\varepsilon(\theta) \alpha_2}{\lambda_2} \right)^{\frac{1}{1+\varepsilon(\theta)}} - 1 \right]. \quad (65)$$

Under Condition C5, the average power of RRH 1 and RRH 2 are respectively given by

$$T_{\text{RRH1}}^{\text{C5}} = \frac{P_1^{\text{peak}}}{\Gamma(m)} \int_{\tilde{\alpha}_2^l}^{\tilde{\alpha}_2^u} \left[\gamma\left(m, \frac{mB}{\bar{\alpha}_1}\right) - \gamma\left(m, \frac{m\lambda_1 \alpha_2}{\bar{\alpha}_1 \lambda_2}\right) \right] f(\alpha_2) d\alpha_2, \quad (66)$$

$$T_{\text{RRH2}}^{\text{C5}} = J_1 - J_2 \quad (67)$$

with

$$J_1 = \frac{1}{\Gamma(m)} \int_{\tilde{\alpha}_2^l}^{\tilde{\alpha}_2^u} C \left(\gamma\left(m, \frac{mB}{\bar{\alpha}_1}\right) - \gamma\left(m, \frac{m\lambda_1 \alpha_2}{\bar{\alpha}_1 \lambda_2}\right) \right) f(\alpha_2) d\alpha_2$$

$$J_2 = \frac{\bar{\alpha}_1 P_1^{\text{peak}}}{m\Gamma(m)} \int_{\tilde{\alpha}_2^l}^{\tilde{\alpha}_2^u} \frac{1}{\alpha_2} (E - G) f(\alpha_2) d\alpha_2,$$

where E and G are respectively given by

$$E = \gamma\left(m+1, \frac{mB}{\bar{\alpha}_1}\right), G = \gamma\left(m+1, \frac{m\lambda_1 \alpha_2}{\bar{\alpha}_1 \lambda_2}\right)$$

with B defined in (57), $\tilde{\alpha}_2^l$ and $\tilde{\alpha}_2^u$ are the solutions of $h(\alpha_2) = 0$ with a, b, c defined in (59).

On the other hand, when the third condition in Lemma 3 is satisfied, inequality (63) holds for $0 \leq \alpha_2 \leq \alpha_2^l$ or $\alpha_2 \geq \alpha_2^u$, where α_2^l and α_2^u are the solutions of $h(\alpha_2) = 0$ with a, b, c defined in (52). Additionally, it is easy to verify that the curve of $h(\alpha_2)$ associated with a, b, c defined in (52) is above the curve of $h(\alpha_2)$ with a, b, c defined in (59). Hence, the following relations hold:

$$\tilde{\alpha}_2^l < \alpha_2^l < \alpha_2^u < \tilde{\alpha}_2^u. \quad (68)$$

Combining (68) with condition (58), the feasible region of α_2 is given by

$$\tilde{\alpha}_2^l < \alpha_2 < \alpha_2^l, \alpha_2^u < \alpha_2 < \tilde{\alpha}_2^u. \quad (69)$$

As a result, when the following conditions are satisfied with a, b, c defined in (52):

$$C6 : C_X, ab - c < 0 \text{ and } \left(\frac{c}{ab} \right)^{1/(b-1)} (1-b) + b < 0, \quad (70)$$

the average power required for RRH 1 and RRH 2, denoted as $T_{\text{RRH1}}^{\text{C6}}$ and $T_{\text{RRH2}}^{\text{C6}}$ respectively, is similar to the expressions of $T_{\text{RRH1}}^{\text{C5}}$ and $T_{\text{RRH2}}^{\text{C5}}$ except that the integration interval of α_2 becomes (69).

Case II: If the following condition is satisfied:

$$\frac{\lambda_1}{\lambda_2} \alpha_2 < A, \quad (71)$$

the feasible region of α_1 is $B > \alpha_1 > A$, where B is defined in (57). The above condition is equivalent to $h(\alpha_2) < 0$ with a, b, c defined in (52). To guarantee the existence of a positive α_2 , the third condition in Lemma 3 should be satisfied.

⁴Under Condition C5, a, b, c are defined in (59).

TABLE II
MAIN RESULTS WHEN $I = 2$, AND $\frac{\lambda_1}{\alpha_1} \leq \frac{\lambda_2}{\alpha_2}$

	Conditions	Average Power
$ \mathcal{I}' = 1$	C1	$T_{\text{RRH}_1}^{\text{C1}}$
	C2	$T_{\text{RRH}_1}^{\text{C2}}$
	C3	$T_{\text{RRH}_1}^{\text{C3}}$
$ \mathcal{I}' = 2$	C4	$T_{\text{RRH}_1}^{\text{C4}}, T_{\text{RRH}_2}^{\text{C4}}$
	C5	$T_{\text{RRH}_1}^{\text{C5}}, T_{\text{RRH}_2}^{\text{C5}}$
	C6	$T_{\text{RRH}_1}^{\text{C6}}, T_{\text{RRH}_2}^{\text{C6}}$
	C7	$T_{\text{RRH}_1}^{\text{C7}}, T_{\text{RRH}_2}^{\text{C7}}$

Assuming that this condition is satisfied, the feasible region of α_2 is given by $\alpha_2^l < \alpha_2 < \alpha_2^u$, where α_2^l and α_2^u are the solutions of $h(\alpha_2) = 0$ with a, b, c defined in (52). Again, by using the relations in (68) and the condition (58), the feasible region of α_2 is given by $\alpha_2^l < \alpha_2 < \alpha_2^u$.

Hence, if the following conditions are satisfied with a, b, c defined in (52):

$$C7: C_X, ab - c < 0 \text{ and } \left(\frac{c}{ab}\right)^{1/(b-1)}(1-b) + b < 0, \quad (72)$$

that the average powers required for RRH 1 and RRH 2 are respectively given by

$$\frac{T_{\text{RRH}_1}^{\text{C7}}}{\Gamma(m)} \int_{\alpha_2^l}^{\alpha_2^u} \left[\gamma\left(m, \frac{mB}{\alpha_1}\right) - \gamma\left(m, \frac{mA}{\alpha_1}\right) \right] f(\alpha_2) d\alpha_2, \quad (73)$$

$$T_{\text{RRH}_2}^{\text{C7}} = \tilde{J}_1 - \tilde{J}_2, \quad (74)$$

where \tilde{J}_1 and \tilde{J}_2 are given by

$$\tilde{J}_1 = \frac{1}{\Gamma(m)} \int_{\alpha_2^l}^{\alpha_2^u} C\left(\gamma\left(m, \frac{mB}{\alpha_1}\right) - \gamma\left(m, \frac{mA}{\alpha_1}\right)\right) f(\alpha_2) d\alpha_2,$$

$$\tilde{J}_2 = \frac{\alpha_1 P_1^{\text{peak}}}{m\Gamma(m)} \int_{\alpha_2^l}^{\alpha_2^u} \frac{1}{\alpha_2} (H - L) f(\alpha_2) d\alpha_2.$$

where H and L are respectively given by

$$H = \gamma\left(m + 1, \frac{mB}{\alpha_1}\right), L = \gamma\left(m + 1, \frac{mA}{\alpha_1}\right).$$

C. Discussion of the results

In this subsection, we summarize the results discussed in the above two subsections in Table II. The average power required for each RRH contributed under condition (23) is given by

$$P_{\text{RRH}_1}^{\frac{\lambda_1 \leq \lambda_2}{\alpha_1 \leq \alpha_2}} = \sum_{i=1}^7 T_{\text{RRH}_1}^{\text{Ci}} \varepsilon(\text{Ci}), P_{\text{RRH}_2}^{\frac{\lambda_1 \leq \lambda_2}{\alpha_1 \leq \alpha_2}} = \sum_{i=4}^7 T_{\text{RRH}_2}^{\text{Ci}} \varepsilon(\text{Ci}), \quad (75)$$

where $\varepsilon(\cdot)$ is an indicator function, defined as

$$\varepsilon(\text{Ci}) = \begin{cases} 1, & \text{if Condition Ci holds,} \\ 0, & \text{otherwise.} \end{cases} \quad (76)$$

Then, the average power required for each RRH is given by

$$P_{\text{RRH}_1} = P_{\text{RRH}_1}^{\frac{\lambda_1 \leq \lambda_2}{\alpha_1 \leq \alpha_2}} + P_{\text{RRH}_1}^{\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}}, P_{\text{RRH}_2} = P_{\text{RRH}_2}^{\frac{\lambda_1 \leq \lambda_2}{\alpha_1 \leq \alpha_2}} + P_{\text{RRH}_2}^{\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}}, \quad (77)$$

where $P_{\text{RRH}_1}^{\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}}$ and $P_{\text{RRH}_2}^{\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}}$ denotes the average transmit power under condition $\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}$ for RRH 1 and RRH 2, which can be calculated as the condition of $\frac{\lambda_1 \leq \lambda_2}{\alpha_1 \leq \alpha_2}$.

To provide more insights concerning the joint power allocation results for the case of $I = 2$, in Fig. 4 we plot the regions corresponding to different cases of the dual variables. For clarity, we only consider the case of $\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}$.

Fig. 4-(a) corresponds to the case of $\lambda_1 = \lambda_2 = 1$. From this figure, we can see that our proposed joint power allocation

algorithm divides the region of $\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}$ into two exclusive regions by the solid lines. If (α_1, α_2) falls into the region T_1 , both RRHs remain silent. On the other hand, if (α_1, α_2) falls into T_2 , Condition C2 is satisfied and only RRH 1 will transmit with positive power, but less than the peak power.

Fig. 4-(b) corresponds to the case of $\lambda_1 = 1/5, \lambda_2 = 1$. In this case, the region of $\frac{\lambda_1 > \lambda_2}{\alpha_1 > \alpha_2}$ is divided into five exclusive regions. Similarly, in region T_1 , none of the RRHs transmit. In region T_2 and T_4 , Condition C3 is satisfied and only RRH 1 is assigned non-zero power for data transmission, but less than the peak power. If (α_1, α_2) falls into region T_3 , Condition C1 is satisfied, and RRH 1 will transmit at peak power and RRH 2 still remains silent. However, if (α_1, α_2) falls into the region T_5 , Condition C5 holds, RRH 1 will transmit at peak power and RRH 2 is allocated positive power that is lower than the peak power.

Fig. 4-(c) corresponds to the case of $\lambda_1 = \lambda_2 = 1/10$. In this case, the region is partitioned into as many as eight regions. Regions T_1 - T_4 are the same as the case in Fig. 4-(b). If (α_1, α_2) falls into regions T_6 and T_8 , Conditions C6 is satisfied, hence RRH 1 will transmit at its peak power and RRH 2 is assigned non-zero power for its transmission, but its power is less than the peak power. If (α_1, α_2) falls into region T_7 , Condition C7 is satisfied. Similarly, RRH 1 transmits at its maximum power and RRH 2 transmits at a non-zero power below its peak power. On the other hand, if (α_1, α_2) falls into region T_7 , Condition C4 is satisfied and both RRHs will transmit at their peak power.

It is interesting to find that with the reduction of the dual variables, more RRHs will transmit at non-zero power or even the peak power. This can be explained as follows. The dual variables can be regarded as a pricing factor, where a lower dual variable will encourage the RRHs to be involved in transmission due to the low cost.

V. POWER ALLOCATION IN EXTREME CASES

In this section, we discuss the power allocation for two extreme cases: 1) when $\theta \rightarrow 0$, representing no delay requirement; 2) when $\theta \rightarrow \infty$ and $P_i^{\text{peak}} \rightarrow \infty, \forall i \in \mathcal{I}$, representing the extremely strict zero delay requirement.

A. $\theta \rightarrow 0$ (No delay requirements)

When $\theta \rightarrow 0$, the system is delay-tolerant. The EC maximization problem is equivalent to the ergodic capacity maximization problem, which is given by

$$\begin{aligned} \max_{\{p_i(\alpha), \forall i\}} & \mathbb{E}_{\alpha} [\log_2 (1 + \sum_{i \in \mathcal{I}} p_i(\alpha) \alpha_i)] \\ \text{s.t.} & \mathbb{E}_{\alpha} [p_i(\alpha)] \leq P_i^{\text{avg}}, \forall i \\ & 0 \leq p_i(\alpha) \leq P_i^{\text{peak}}, \forall i. \end{aligned} \quad (78)$$

By using a similar method as in Section III, the optimal transmit power at each RAU is given by

$$P_{\pi(a)}^* = \begin{cases} P_{\pi(a)}^{\text{peak}}, & a < |\mathcal{I}'|; \\ \min \left\{ P_{\pi(|\mathcal{I}'|)}^{\text{peak}}, \tilde{T}_{\pi(a)} \right\}, & a = |\mathcal{I}'|; \\ 0, & a > |\mathcal{I}'|; \end{cases} \quad (79)$$

where $\tilde{T}_{\pi(a)}$ is given by

$$\tilde{T}_{\pi(a)} = \frac{1}{\alpha_{\pi(|\mathcal{I}'|)}} \left(\frac{1}{\ln 2} \cdot \frac{\alpha_{\pi(|\mathcal{I}'|)}}{\lambda_{\pi(|\mathcal{I}'|)}} - \sum_{a=1}^{|\mathcal{I}'|-1} P_{\pi(a)}^{\text{peak}} \alpha_{\pi(a)}^{-1} \right)$$

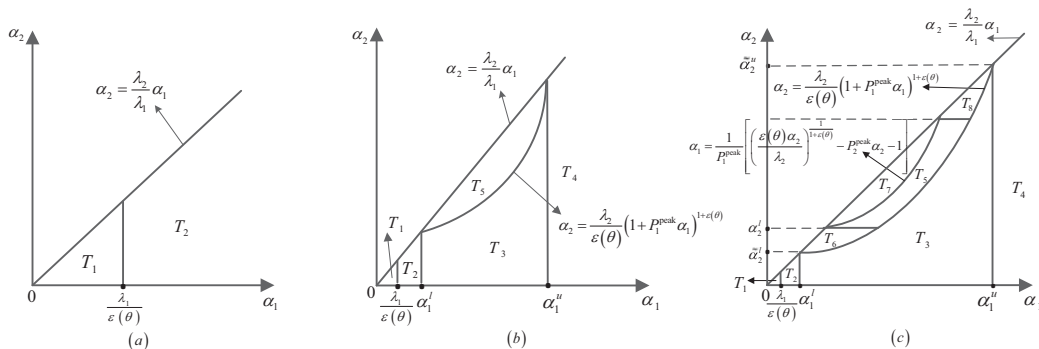


Fig. 4. The partitions of the region of $\frac{\lambda_1}{\alpha_1} > \frac{\lambda_2}{\alpha_2}$ under different dual variables: (a) $\lambda_1 = \lambda_2 = 1$; (b) $\lambda_1 = 1/5, \lambda_2 = 1$; (c) $\lambda_1 = \lambda_2 = 1/10$. The system parameters are set as [11]; Time frame of length $T_f = 0.2$ ms, the system bandwidth $B = 100$ KHz, delay QoS exponent $\theta = (\ln 2)/20$ so that $\epsilon(\theta) = 1$, peak power constraint $P_i^{\text{peak}} = 1$ W, $\forall i = 1, 2$.

with $|\mathcal{I}'|$ being the largest value of x such that

$$\frac{1}{\ln 2} \cdot \frac{\alpha_{\pi(x)}}{\lambda_{\pi(x)}} > 1 + \sum_{a=1}^{x-1} P_{\pi(a)}^{\text{peak}} \alpha_{\pi(a)} \quad (80)$$

and π is a permutation over \mathcal{I} so that $\frac{\lambda_{\pi(i)}}{\alpha_{\pi(i)}} \leq \frac{\lambda_{\pi(j)}}{\alpha_{\pi(j)}}$, when $i < j, i, j \in \mathcal{I}$.

When there is only one RRH, the optimal power allocation reduces to the conventional water-filling solution that is given by

$$p_1^* = \left[\frac{1}{\lambda_1 \ln 2} - \frac{1}{\alpha_1} \right]_0^{P_1^{\text{peak}}}, \quad (81)$$

where $[x]_0^y$ represents that the value is zero if $x < 0$, x if $0 < x < y$, and y if $x > y$.

B. $\theta \rightarrow \infty$ and $P_i^{\text{peak}} \rightarrow \infty, \forall i \in \mathcal{I}$ (Extremely strict delay requirement)

For this case, the system cannot tolerate any delay, and the EC is equal to the zero-outage capacity. Hence, the optimal power allocation for each RRH reduces to the channel inversion associated with a fixed data rate [28] given by

$$p_i^* = \frac{\beta_i}{\alpha_i}, \forall i \in \mathcal{I}, \quad (82)$$

where β_i is specifically selected to satisfy the average power constraints. For the Nakagami- m channel defined in (1), we have

$$\mathbb{E}_{\alpha_i} \left\{ \frac{1}{\alpha_i} \right\} = \begin{cases} \frac{m}{(m-1)\bar{\alpha}_i}, & m > 1 \\ 0, & 1 \geq m. \end{cases} \quad (83)$$

Then, β_i can be calculated as

$$\beta_i = \begin{cases} \frac{(m-1)\bar{\alpha}_i P_i^{\text{avg}}}{m}, & m > 1 \\ 0, & 1 \geq m. \end{cases} \quad (84)$$

The EC can be obtained as

$$\text{EC} = \begin{cases} T_f B \log_2(1 + \sum_{i \in \mathcal{I}} \beta_i), & m > 1 \\ 0, & 1 \geq m. \end{cases} \quad (85)$$

Note that when $m = 1$, the EC is equal to zero, which is consistent with the result in [28], namely that the zero-outage capacity for Rayleigh fading is equal to zero. However, when $m > 1$, the EC increases with m . This coincides with the intuition that with the increase of m , the channel variations reduce and the channel becomes more stable. As a result, the queue-length variations are reduced and hence higher delay requirements can be satisfied.

VI. EXTENSION TO THE MULTIUSER CASE

The above sections focus on the single user case. However, in C-RAN, due to the powerful computational capability of the BBU pool, C-RAN is designed with the goal of serving multiple users. To simplify the analysis, we assume that the RRHs transmit the signals to different users in orthogonal channels to avoid multiuser interference. Similar assumptions have been made in [22], [23], [29], [30].

Let us denote the total number of users by K and $\mathcal{K} = \{1, \dots, K\}$. The QoS exponent for user k is denoted as θ_k , and the set of QoS exponents is denoted as $\boldsymbol{\theta} = \{\theta_1, \dots, \theta_K\}$. The channel's power gain from RRH i to user k is denoted as $\alpha_{i,k}$. The set of channel gains from all RRHs to user k is denoted as $\boldsymbol{\alpha}_k = \{\alpha_{1,k}, \dots, \alpha_{I,k}\}$. The set of all channel gains in the network is denoted as $\boldsymbol{\alpha} = \{\boldsymbol{\alpha}_1, \dots, \boldsymbol{\alpha}_K\}$. For simplicity, the peak power constraints are not considered. We aim for optimizing the power allocation to max

$$\max_{\{p_{i,k}(\boldsymbol{\nu}), \forall i, k\}} \sum_{k \in \mathcal{K}} \frac{1}{T_f B \theta_k} \log \left(\mathbb{E}_{\boldsymbol{\alpha}} \left[e^{-\theta_k R_k(\boldsymbol{\nu})} \right] \right) \quad (86a)$$

$$\text{s.t.} \quad \mathbb{E}_{\boldsymbol{\alpha}} \left[\sum_{k \in \mathcal{K}} p_{i,k}(\boldsymbol{\nu}) \right] \leq P_i^{\text{avg}}, \forall i \in \mathcal{I}, \quad (86b)$$

$$0 \leq p_{i,k}(\boldsymbol{\nu}), \forall i \in \mathcal{I}, k \in \mathcal{K}, \quad (86c)$$

where $\boldsymbol{\nu} = \{\boldsymbol{\alpha}, \boldsymbol{\theta}\}$ represents the network condition that includes both the channel's power gains and the QoS exponent requirements, $R_k(\boldsymbol{\nu})$ is the data rate achieved by user k that is given by $R_k(\boldsymbol{\nu}) = T_f B \log_2(1 + \sum_{i \in \mathcal{I}} p_{i,k}(\boldsymbol{\nu}) \alpha_{i,k})$.

Note that in the multiuser case, each user's power allocation depends both on its own channel condition and on its own delay requirement as well as those of other users'. Furthermore, the power allocation solution of each user is coupled with the per-RRH average power constraints, which complicates the analysis. Unlike in the single user case, Problem (86) cannot be decomposed into several independent subproblems for each channel fading state. The reason for this is that the objective function in Problem (86) cannot be transformed into the format of Problem (7). However, since the EC is a concave function [31] and the constraints are linear, Problem (86) still remains a convex optimization problem. Hence, the Lagrangian duality method can still be used to solve this problem.

Specifically, we introduce the dual variables of $\lambda_i, \forall i$, and $\delta_{i,k}, \forall i, k$ for the corresponding constraints in Problem (86). The KKT conditions for the optimal solutions of Problem (86)

are given by

$$-\frac{\varepsilon(\theta_k)\alpha_{i,k}Z_k(\boldsymbol{\nu})^{-\varepsilon(\theta_k)-1}}{\kappa_k}f(\boldsymbol{\alpha})+\lambda_i f(\boldsymbol{\alpha})-\delta_{i,k}=0, \forall i \quad (87a)$$

$$\lambda_i \left(\mathbb{E}_{\boldsymbol{\alpha}} \left[\sum_{k \in \mathcal{K}} p_{i,k}^*(\boldsymbol{\nu}) \right] - P_i^{\text{avg}} \right) = 0, \forall i \quad (87b)$$

$$\delta_{i,k}^* p_{i,k}^*(\boldsymbol{\nu}) = 0, \forall i, k \quad (87c)$$

$$p_{i,k}^*(\boldsymbol{\nu}) \geq 0, \forall i, k \quad (87d)$$

where $f(\boldsymbol{\alpha})$ represents the joint PDF of $\boldsymbol{\alpha}$, $Z_k(\boldsymbol{\nu}) = 1 + \sum_{i \in \mathcal{I}} p_{i,k}^*(\boldsymbol{\nu})\alpha_{i,k}$ and $\varepsilon(\theta_k) = \theta_k T_f B / \ln 2$, κ_k is given by

$$\kappa_k = T_f B \theta_k \mathbb{E}_{\boldsymbol{\alpha}} \left[Z_k(\boldsymbol{\nu})^{-\varepsilon(\theta_k)} \right]. \quad (88)$$

To satisfy the above KKT conditions, we first find the optimal power allocation associated with the fixed dual variables $\lambda_i, \forall i$, then update the dual variables by using the sub-gradient method.

Given $\lambda_i, \forall i$, we then have the following theorem.

Theorem 3: There is at most one RRH serving each user and the index of this RRH is given by

$$i^* = \arg \min_{i \in \mathcal{I}} \frac{\lambda_i}{\alpha_{i,k}}, \quad (89)$$

while the corresponding power allocation is given by

$$p_{i^*,k}^* = \left[\left(\frac{\varepsilon(\theta_k)}{\kappa_k \lambda_{i^*}} \right)^{\frac{1}{1+\varepsilon(\theta_k)}} - \frac{\varepsilon(\theta_k)}{\alpha_{i^*,k}^{1+\varepsilon(\theta_k)}} - \frac{1}{\alpha_{i^*,k}} \right]^+, \quad (90)$$

where $[x]^+ = \max\{0, x\}$.

Proof: The proof is similar to that of the single user scenario of Section III, which is omitted for simplicity. ■

Although each user is served by only one RRH for each channel state, they still benefit from the multi-RRH diversity, as seen in (89). Similarly, the online calculation method used for the single user case can be adopted to approximate the value of κ_k .

VII. SIMULATIONS

In this section, we characterize the performance of our proposed algorithm. We consider a C-RAN network covering a square area of 2 km \times 2 km. The user is located at the center of this region and the RRHs are independently and uniformly allocated in this area. Unless otherwise stated, we adopt the same simulation parameters as in [11]: Time frame of length $T_f = 0.1$ ms; system bandwidth of $B = 200$ KHz; average power constraint of $P_i^{\text{avg}} = 0.5$ W, $\forall i$; peak power constraint of $P_i^{\text{peak}} = 1$ W, $\forall i$; QoS exponent of $\theta = 0.05$; Nakagami fading parameter $m = 2$. The path-loss is modeled as $PL_i = 148.1 + 37.6 \log_{10} d_i$ (dB) [32], where d_i is the distance between the i th RRH and the user measured in km. The channel also includes the log-normal shadowing fading with zero mean and 8 dB standard derivation. The noise density power is -174 dBm/Hz [32].

We compare our algorithm to the following algorithms:

1) *Nearest RRH serving algorithm:* In this algorithm, the user is only served by its nearest RRH, and the optimization method proposed in [11] for point-to-point systems is adopted to solve the power allocation problem in this setting. This algorithm is proposed to show the benefits of cooperative transmission in C-RAN.

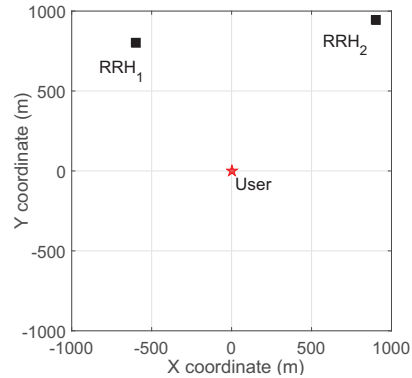


Fig. 5. Random network topology with two RRHs. The user is located at the center of the C-RAN. The coordinates of RRH 1 and RRH 2 are given by $[-600, 800]$ and $[900, 946]$, respectively. The CPNRs are $\bar{\alpha}_1 = 3.89$ and $\bar{\alpha}_2 = 1.43$.

2) *Constant power allocation algorithm:* In this algorithm, the transmit power is set to be equal to the average power constraint for any time slots. Since the peak power limit is higher than the average power limit, both the average power constraints and peak power constraints can be satisfied. This approach was assumed to illustrate the benefits of dynamic power allocation proposed in this paper.

3) *Independent power allocation algorithm:* In this algorithm, each RRH i independently optimizes its power allocation without considering the joint channel conditions of the other RRHs. The optimization problem is given by

$$\max_{p_i(\boldsymbol{\nu})} -\frac{1}{\theta} \log \left(\mathbb{E}_{\boldsymbol{\alpha}} \left[e^{-\theta T_f B \log_2(1+p_i(\boldsymbol{\nu})\alpha_i)} \right] \right) \quad (91a)$$

$$\text{s.t. } \mathbb{E}_{\boldsymbol{\alpha}} [p_i(\boldsymbol{\nu})] \leq P_i^{\text{avg}}, \quad (91b)$$

$$0 \leq p_i(\boldsymbol{\nu}) \leq P_i^{\text{peak}}. \quad (91c)$$

The optimal power allocation solution is given by (18). This algorithm is invoked for showing the benefits of jointly optimizing the power allocation according to the joint channel conditions of all RRHs.

4) *Ergodic capacity maximization algorithm:* This algorithm aims for maximizing the ergodic capacity without considering the delay requirement. The optimal power allocation solution is given by (79).

5) *Channel inversion algorithm:* This algorithm imposes an extremely strict delay requirement. The power allocation is the channel inversion given by (82).

In the following, we first consider the case of $I = 2$, where the average power required for each RRH can be numerically obtained according to the results of Section IV. Then, we study the more general case associated with more than two RRHs.

Fig. 5 shows a randomly generated network topology relying on two RRHs. The average CPNRs related to RRH 1 and RRH 2 are then given by $\bar{\alpha}_1 = 3.89$ and $\bar{\alpha}_2 = 1.43$. Figs. 6-8 are based on this network topology. In this setting, the user is only served by RRH 1 due to its shorter distance compared to RRH 2, when using the nearest RRH algorithm.

In Fig. 6, we study the convergence behaviour of the proposed algorithm under different delay exponents and step-size parameters. The left three subplots correspond to the QoS exponent $\theta = 0.005$, while the right three correspond to $\theta = 0.05$. It can be observed from this figure that the

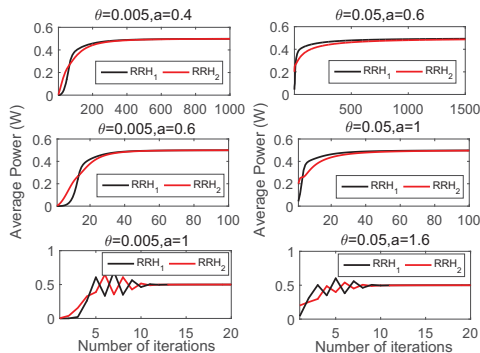


Fig. 6. Convergence behaviour of the proposed algorithm for the special case of two RRHs under different step parameters. Left three subplots correspond to the QoS exponent $\theta = 0.005$, and the right three correspond to $\theta = 0.05$.

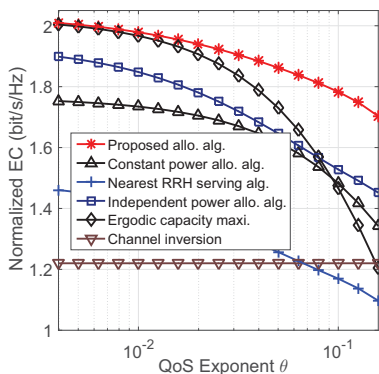


Fig. 7. Normalized EC for various algorithms vs QoS exponent θ .

convergence speed mainly depends on step-size parameter a . For both cases of θ , a smaller step-size parameter leads to slower convergence and larger one leads to faster convergence speed. For example, for the case of $\theta = 0.005$, nearly 700 iterations are required for convergence when $a = 0.4$, while only 20 iterations are needed when $a = 1$. However, since the subgradient method is not an ascent method, a larger value of a may lead to a fluctuation of the power value. A small value of a yields a smooth but slow convergence. Hence, the step-size parameter should be carefully chosen to strike a tradeoff between the convergence speed and the smoothness of the power curve. It should be emphasized that the main advantage for the case of two RRHs is that the Lagrange dual variables can be calculated in an off-line manner by using the results of Section IV, and stored in the memory.

Let us now study the impact of the delay requirements on the EC performance for various algorithms in Fig. 7. The normalized EC performance (which is defined as the

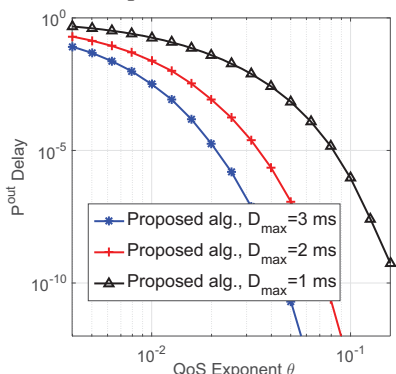


Fig. 8. Delay-outage probability versus QoS exponent θ for various values of D_{\max} for our proposed algorithm.

EC divided by B and T_f with the unit of ‘bit/s/Hz’) is considered. As expected, when the delay-QoS requirement becomes more stringent, i.e., the value of QoS exponent θ increases, the normalized EC achieved by all algorithms is reduced. By employing two RRHs for jointly serving the user to exploit higher spatial degrees of freedom, the proposed algorithm significantly outperforms the nearest RRH based algorithm, where only one RRH is invoked for transmission. For example, for $\theta = 0.1$ the normalized EC provided by the former algorithm is roughly 50% higher than that of the latter algorithm. It is observed that the performance of the latter algorithm is even inferior to that of the naive constant power allocation algorithm. Since our proposed algorithm adapts its power allocation to delay-QoS requirement, whilst additionally taking into account the channel conditions, it achieves a higher normalized EC than the constant power allocation algorithm, and the performance gain attained is about 20% when $\theta = 0.1$. By optimizing the power allocation based on the joint channel conditions, the proposed algorithm performs better than the independent one, where the joint relationship of the channel conditions is ignored. The performance gain is more prominent when the delay-QoS requirement is very stringent, which can be up to 18.6% in this example. The proposed algorithm has similar performance to that of the ergodic capacity maximization algorithm for small θ , while the performance gain provided by the proposed algorithm becomes higher for a large θ . For a high θ , the normalized EC achieved by the ergodic capacity maximization algorithm is even lower than that of the constant power allocation algorithm. It is seen from Fig. 7 that the performance of the channel inversion based power allocation method is much worse than that of our proposed algorithm, since it aims for an extremely strict delay budget rather than adaptively adjusting the power allocation according to the delay requirements.

Fig. 8 shows the delay-outage probability versus QoS exponent θ for various values of D_{\max} for our proposed algorithm. In this example, the UL and DL transmission duration and the fronthaul delay are set as $D_T = D_F = T_f = 0.1$ ms [33]. Then, the corresponding queuing delay is given by $D_q = D_{\max} - D_T - D_F = D_{\max} - 0.2$ ms. The maximum incoming data rate is set to be equal to the EC, i.e. to $\mu = \text{EC}(\theta)$. The method in [6] is used for calculating the delay-outage probability. As expected, the delay outage probability increases with the reduction of D_{\max} . By appropriately choosing the QoS exponent θ , the delay outage probability can be reduced below 10^{-8} . For example, for the case of $D_{\max} = 1$ ms, the delay outage probability is as low as 4×10^{-10} when $\theta = 0.1585$, which satisfies the stringent delay requirement of the ultra-reliable low latency communications (URLLC) in 5G [1]. For a given target $P_{\text{delay}}^{\text{out}}$, the corresponding value of θ obtained from Fig. 8 can be used in Fig. 7 to find the achievable EC. For example, when the delay outage probability requirement is $P_{\text{delay}}^{\text{out}} = 10^{-6}$ for the case of $D_{\max} = 1$ ms, the corresponding θ is given by 0.1. The resultant normalized EC becomes 1.78 bit/s/Hz according to Fig. 7.

We now consider a more general case in Fig. 9, where five RRHs are randomly located in a square. The average CPNRs received from these RRHs are then $\bar{\alpha}_1 = 64.3$, $\bar{\alpha}_2 = 5.3$,

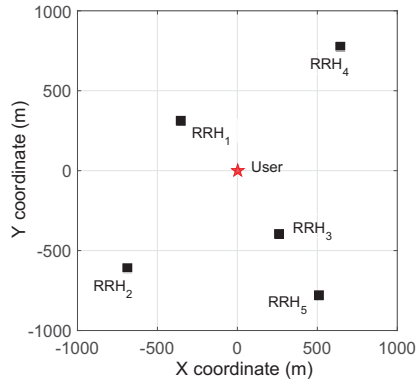


Fig. 9. Random network topology with five RRHs.

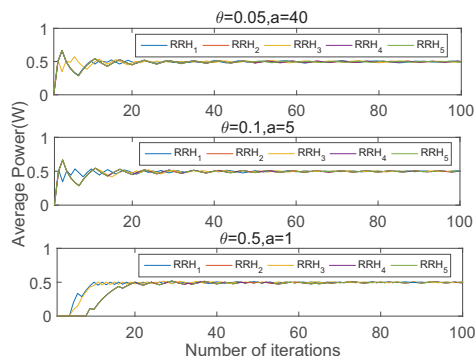


Fig. 10. Convergence behaviour of the online tracking method.

$\bar{\alpha}_3 = 63.1$, $\bar{\alpha}_4 = 3.8$ and $\bar{\alpha}_5 = 5.1$.

Based on Fig. 9, the convergence behaviour of the online tracking method is shown in Fig. 10, where different QoS requirements are tested. As shown in Fig. 10, the online tracking method converges promptly for all the values of θ considered which is achieved by properly choosing the step parameter a . These observations demonstrate the efficiency of the online tracking method. In Fig. 11, we plot the effective capacity performance for various algorithms for this more general scenario. Similar observations can be found from this figure. For example, the normalized EC achieved by all algorithms decrease with the QoS exponent θ , and the proposed algorithm significantly outperform the other algorithms.

Finally, we study the EC performance of the multiuser scenario. The simulation setup is given in Fig. 12, where there are two users located at $[-100, 0]$ and $[0, 100]$, respectively, while the locations of the four RRHs are given by $[650, 650]$, $[-650, 650]$, $[-650, -650]$, and $[650, -650]$. We should em-

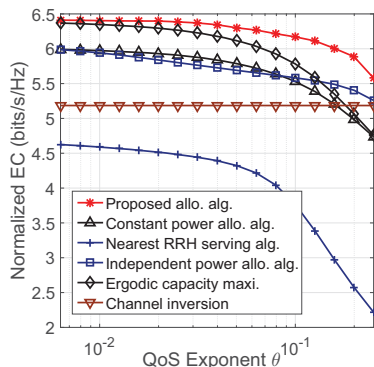


Fig. 11. Normalized EC for various algorithms vs QoS exponent θ for the more general case of $I = 5$.

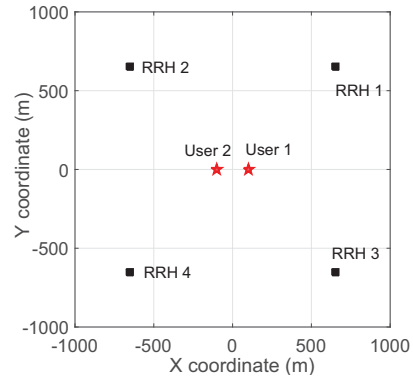


Fig. 12. Simulated network topology for two users with four RRHs.

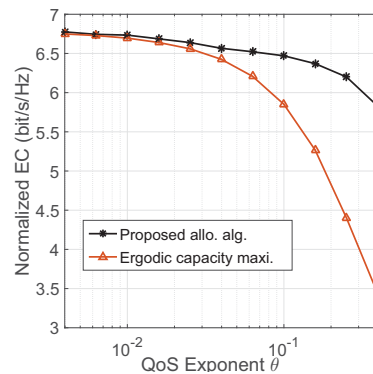


Fig. 13. The sum normalized EC for various algorithms vs QoS delay exponent θ .

phasize that our algorithm used for the multiuser scenario is applicable for any network setup. In Fig. 13, we compare our proposed EC maximization algorithm of Subsection VI to the multiuser ergodic capacity maximization algorithm in terms of the sum EC of the two users. Note that a similar performance trend has been observed to that in Fig. 7. For example, both algorithms have almost the same performance in the low QoS exponent regime, while our proposed EC-oriented algorithm performs much better than the ergodic capacity-oriented algorithm for high exponents. When $\theta = 0.4$, the performance gain is up to 2.3 bit/s/Hz.

VIII. CONCLUSIONS

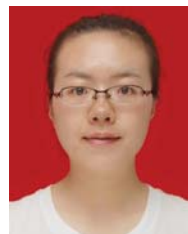
We considered joint power allocation for the EC maximization of C-RAN, where the user has to guarantee a specific delay-QoS requirement to declare successful transmission. Both the per-RRH average and peak power constraints were considered. We first showed that the EC maximization problem can be equivalently transformed into a convex optimization problem, which was solved by using the Lagrange dual decomposition method and by studying the KKT conditions. The online tracking method was proposed for calculating the average power for each RRH. For the special case of two RRHs, the expression of average power for each RRH can be obtained in closed-form. We also provided the power allocation solutions for the extreme cases of $\theta \rightarrow \infty$ and $\theta \rightarrow 0$. The simulation results showed that our proposed algorithm converges promptly and performs much better than the existing algorithms, including the conventional ergodic capacity maximization method operating without delay requirements. A delay outage probability of 10^{-9} can be achieved at $D_{\max} = 1$

ms by our proposed algorithm through controlling the value of θ , which is very promising for the applications in future URLLC in 5G.

In this paper, we only extend the single-user case to the multiple-user interference-free case. For the more general case where each user suffers from the multi-user interference, the formulated optimization problem is non-convex, where the Lagrangian duality method is not applicable. How to deal with this problem will be left for future work. In addition, the fronthaul capacity is generally limited due to the fast oversampled real-time I/Q digital data streams transmitting over the fronthaul links. How to design the transmission scheme by taking into account this constraint will also be considered in the future work.

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